

## ORIGINAL PAPER

# An SMLB-based OFDM receiver over impulsive noise environment

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*The impulsive noise (IN) damages the performance of wireless communication in modern 5G scenarios such as manufacturing and automatic factories. The proposed receiver utilizes constant false alarm rate to obtain the threshold and combines with blanking to further improve the performance of the conventional blanking scheme with acceptable complexity. The simulated results show that the proposed receiver can achieve a lower bit error rate even if the probability of IN occurrence is very high and the power of the IN is much larger than that of the background noise.*

**Keywords:** Impulsive noise, OFDM, 5G, Blanking

Received 27 June 2020; Revised 21 October 2020

## 1. INTRODUCTION

Nowadays, to satisfy the requirement of ubiquitous wireless communications anytime, anywhere, and anyone, more and more new devices are being developed exponentially [1]. In order to support the data traffic due to more and more devices subscribed, 5G wireless communication is expected to achieve 1000 times high mobile data volume [2]. However, the microwave spectrum allocation cannot satisfy the huge amount of the 5G wireless communication; therefore, the untapped frequency such as the millimeter band (mmWave) is expected to mitigate the burden [3]. Generally, mmWave wireless communication is only analyzed under the background noise. However, the impulsive noise (IN) due to the monitoring applications, ignitions of mobile vehicles [4, 5] also increases the bit error rate (BER) which causes the problem of the connectivity reliability and increases the transmission latency in the event of packet loss [6] in a harsh industrial environment [7, 8] which requires low latency and high reliability. Therefore, it is vital to mitigate the impact of the IN in the ultra-reliable low-latency communication (URLLC) [9, 10].

Orthogonal frequency division multiplexing (OFDM) technology is widely utilized in many wireless applications including ISDB-T [11] and 5G [12]. A OFDM system achieves high spectral efficiency and robustness with multipath fading and IN [13]. However, the IN is unneglectable when the interference power of the IN is very large [13].

Blanking, clipping, and the combination of the blanking and clipping are the conventional methods to reduce the impact of the IN [14–18]. The drawback of these methods is degradation of the performance when the useful signal is mistaken as the IN. Therefore, it is challenging to obtain the optimal threshold in order to judge the true useful signal or the IN. Zhidkov [17] has proposed a method to find the theoretical threshold value and Epple and Schnell [18] further proposed a method using an adaptive threshold to mitigate the impact of the IN. However, these methods require the parameters of the IN model. On the other hand, Miyamoto *et al.* [19] have proposed the maximum likelihood sequence estimation (MLSE) decoding which compares the received signal with all possible candidates and decides the best signal to improve the performance of single carrier systems over the environments with large IN. Although the system delivers good performance, the complexity is very high. Especially, the complexity of OFDM with MLSE increases exponentially with the number of subcarriers. As a matter of fact, SML has been proposed in [20] to improve the performance of OFDM and Hou and Hase [21] further show that SML-based OFDM can reconstruct the original signal even if only successive time-domain symbols are missing due to packet loss and the assumption is that noise only includes additive white Gaussian noise (AWGN) noise.

We propose a OFDM receiver utilizing the combination of suboptimal MLSE and blanking (SMLB) to improve the performance with an acceptable complexity. In addition, the proposed system utilizes constant false alarm rate (CFAR) [22] to obtain the location of the IN by distinguishing the mixed signal including transmitted signal, background noise, and the IN term [23, 24]. On the other hand, suboptimal MLSE (SML) is utilized in the frequency domain to reconstruct the signal after blanking the time-domain

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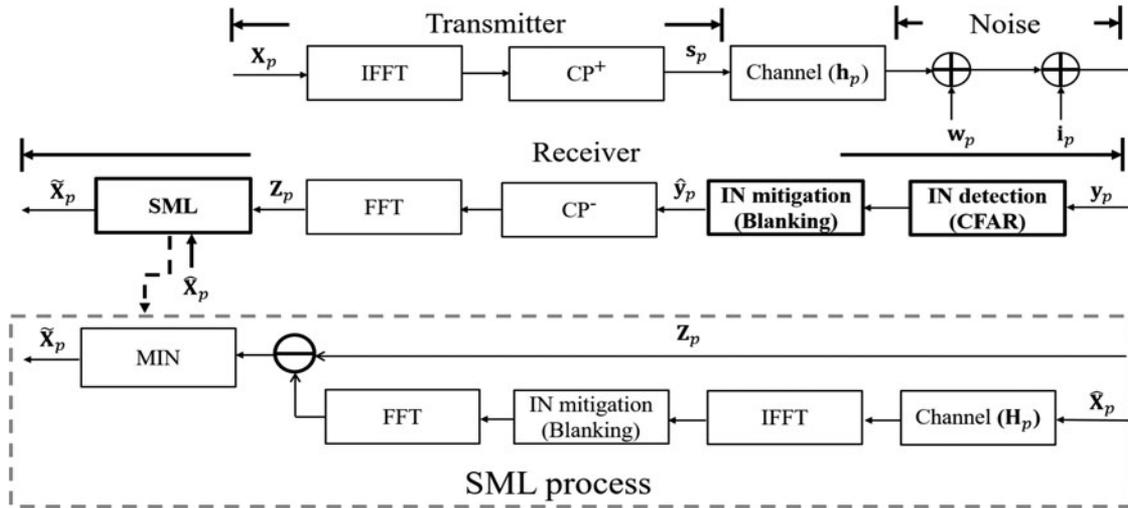


Fig. 1. Structure of the proposed system.

signal. The simulated results show that the proposed system has better performance compared to that of the conventional OFDM with blanking when the power ratio of the IN to the background noise is large in both non-fading and fading channel models.

The remainder of the paper is organized as follows. Section II describes the structure of the system model. The proposed receiver is explained in detail in Section III. Section IV shows the simulated results over the IN environment including the non-multipath and multipath fading channel. Finally, the above-mentioned content is concluded in Section V.

## II. SYSTEM MODEL

Let  $\mathbf{X}_p = [x_p(0), \dots, x_p(N-1)]^T$  represent the M-QAM modulated data stream in the frequency domain with  $N$  subcarriers in the  $p$ th OFDM symbol. As Fig. 1 shows that the modulated data bits are transmitted through inverse fast Fourier transform and cyclic prefix (CP) to obtain the time domain symbols  $\mathbf{s}_p = [s_p(N-N_{cp}), \dots, s_p(N-1), s_p(0), \dots, s_p(N-1)]^T$ . Here  $N_{cp}$  is the length of CP and the power of the transmitted signal  $\sigma_s^2$  is calculated as  $(1/2)E\{|\mathbf{s}_p|^2\}$ .

In this paper, Bernoulli–Gaussian (BG) [25] is utilized as the IN model for the convenience of analyzing the performance of the proposed system. Note that it can be extended to the other famous IN models such as Middleton Class A model, Gaussian mixture model [26, 27]. The noise in this paper is given by

$$\mathbf{n}_p = \mathbf{w}_p + \mathbf{i}_p \quad (1)$$

where  $\mathbf{w}_p = [w_p(0), \dots, w_p(N-1)]^T$  is the background noise and  $\mathbf{i}_p = [i_p(0), \dots, i_p(N-1)]^T$  is the IN which is expressed as

$$i_p(k) = b_p(k) \times g_p(k), \quad k = 0, 1, \dots, N-1. \quad (2)$$

Here,  $g_p(k)$  is the complex white Gaussian noise with zero mean and  $\alpha\sigma_g^2$  variance (i.e.  $\alpha$  shows that how larger the IN is than the background noise).  $b_p(k)$  is the Bernoulli process with probability  $G(b_p(k) = 1) = q$  (i.e.  $G(b_p(k) = 0) = 1 - q$ ). The noise can be generated by the probability density function of the BG which is described as

$$F(\mathbf{n}_p) = (1 - q)\mathcal{N}(\mathbf{n}_p; \mathbf{0}, \sigma_g^2) + q\mathcal{N}(\mathbf{n}_p; \mathbf{0}, \alpha\sigma_g^2) \quad (3)$$

where  $q$  is the probability of the IN occurrence and  $\mathcal{N}(\mathbf{n}_p, \mathbf{0}, \sigma_m^2)$  follows the Gaussian distribution.

## III. PROPOSED RECEIVER

At the receiver side, the received symbols  $\mathbf{y}_p$  are expressed as

$$\mathbf{y}_p = \mathbf{h}_p \otimes \mathbf{s}_p + \mathbf{w}_p + \mathbf{i}_p \quad (4)$$

where  $\mathbf{h}_p = [h_p(0), h_p(1), 0, \dots, 0]^T$  is the channel impulse response for the two-path Rayleigh fading model. If the received symbol's power is greater than the threshold obtained by the CFAR detector, then the symbol is blanked. Here, the threshold can be derived based on the variance of the received symbols  $\sigma_r^2$  and the probability of false-alarm ( $P_{fa}$ ). The assumption of the system is that OFDM signal can be modeled as a complex Gaussian process with Rayleigh envelope distribution when the number of subcarriers is sufficient large [17] in the case of only AWGN exists. Based on [17], the received symbols  $|y_p|$  follow the Rayleigh distribution. The  $P_{fa}$  of  $|y_p|$  is expressed as

$$F_{P_{fa}}(T_B; \sigma_r^2) = e^{(-T_B^2/2\sigma_r^2)}, \quad (5)$$

where  $T_B$  is the blanking threshold. Therefore,  $T_B$  can be obtained as

$$T_B = \sqrt{-2\sigma_r^2 \ln(P_{fa})}, \quad (6)$$

given  $F_{pfa}$ . The blanked symbols are described as

$$\hat{y}_p = \begin{cases} y_p & |y_p| \leq T_B \\ 0 & \text{otherwise} \end{cases} \quad (7)$$

After removing CP and accomplishing FFT, we utilize SML to reconstruct the original symbols. The output of SML can be represented as

$$\tilde{\mathbf{X}}_p = \arg \min |\mathbf{Z}_p - \mathbf{H}_p \hat{\mathbf{X}}_p|^2 \quad (8)$$

with  $\mathbf{Z}_p = [z(0), \dots, z(N-1)]^T$ ,  $\hat{\mathbf{X}}_p = [\hat{x}(0), \dots, \hat{x}(N-1)]^T$  and  $\hat{x}(i) \in \{-1, 1\}$  for BPSK. Here we assume that the channel is perfectly detected. Therefore,  $\mathbf{H}_p$  can be written as

$$\mathbf{H}_p = \begin{bmatrix} H_p(0) & 0 & \dots & 0 \\ 0 & H_p(1) & \dots & 0 \\ \vdots & \vdots & \dots & \vdots \\ 0 & 0 & \dots & H_p(N-1) \end{bmatrix} \quad (9)$$

As we know, the computational complexity of MLSE used in the OFDM system increases exponentially as  $N^P$  with the number of subcarriers  $N$  and the number of constellation subsets  $P$  (i.e.  $P \in \{-1, 1\}$  for BPSK). In order to reduce the complexity, the proposed receiver utilizes SML whose complexity increases linearly as  $MP$  by limiting the candidate constellation points to a given number  $M$  in every iteration.

We define  $\hat{\mathbf{X}}^{(i)(j)}$  as the  $j$ th candidate constellation points of the  $i$ th iteration process. Note that we omit the subscript  $p$  from the above-mentioned parameters for the convenience of analyzing the impact of SML. The steps of SML can be described as follows:

Step 1: Assume that  $P$  is the number of constellation subsets of  $\{-1, 1\}$  for BPSK. We define  $N$  points as  $\hat{\mathbf{X}}^{(1)(u)} = [\hat{x}(0), \dots, \hat{x}(U-1), \dots, 0]$  with  $\hat{x}(k) \in \{-1, 1\}$  and  $k \in [0, \dots, U-1]$ . In other words, there are  $P^U$  kinds of  $\hat{\mathbf{X}}^{(1)(u)}$  (i.e.  $u \in [1, \dots, P^U]$ ). Note that  $U$  denotes the number of candidate constellation points in the first-iteration process.  $\hat{\mathbf{Z}}_u^{(1)} = [z_u^{(1)}(0), \dots, z_u^{(1)}(N-1)]$  are presented as

$$\hat{\mathbf{Z}}_u^{(1)} = \mathbf{H} \hat{\mathbf{X}}^{(1)(u)}. \quad (10)$$

Therefore, the Euclidian distances  $d_u^{(1)}$  between  $\hat{\mathbf{Z}}_u^{(1)}$  and received samples  $\mathbf{Z}$  are evaluated as

$$d_u^{(1)} = \sum_{l=0}^{U-1} |\hat{z}_u^{(1)}(l) - z(l)|. \quad (11)$$

Here there are  $P^U$  kinds of  $\hat{\mathbf{Z}}_u^{(1)}$  generated. After sorting  $d_u^{(1)}$  by ascending order, the corresponding first  $M$  ( $M < P^U$ )  $\hat{\mathbf{Z}}_u^{(1)}$  are selected to continue to the next iteration as  $\hat{\mathbf{Z}}_{(r)}^{(1)}$  ( $r = 1, \dots, M$ ) with corresponding  $\hat{\mathbf{X}}^{(1)(u)}$  which are stored as  $\hat{\mathbf{X}}^{(1)(r)}$  ( $r = 1, \dots, M$ ).

Step 2: Redefine the  $N$  samples  $\hat{\mathbf{X}}^{(2)(u)}$  ( $u = 1, \dots, MP$ ) as  $\hat{\mathbf{X}}^{(2)(u)} = [\hat{\mathbf{X}}^{(1)(r)}, \hat{x}(i), 0, \dots, 0]$  and  $\hat{x}(i) \in \{-1, 1\}$ . Therefore,  $MP$  kinds of vector  $\hat{\mathbf{Z}}_u^{(2)} = [\hat{z}_u^{(2)}(0), \dots, \hat{z}_u^{(2)}(N-1)]$  are presented as

$$\hat{\mathbf{Z}}_u^{(2)} = \mathbf{H} \hat{\mathbf{X}}^{(2)(u)}. \quad (12)$$

The Euclidian distances  $d_u^{(2)}$  ( $u = 0, \dots, MP-1$ ) between  $\hat{\mathbf{Z}}_u^{(2)}$  and the received samples  $\mathbf{Z}$  are evaluated by

$$d_u^{(2)} = \sum_{l=0}^U |\hat{z}_u^{(2)}(l) - z(l)|. \quad (13)$$

The first  $M$   $\hat{\mathbf{Z}}_u^{(2)}$ , which are smaller Euclidian distances, are selected as  $\hat{\mathbf{Z}}_{(r)}^{(2)}$  ( $r = 1, \dots, M$ ) from  $MP$  kinds of  $\hat{\mathbf{Z}}_u^{(2)}$  with corresponding  $\hat{\mathbf{X}}^{(2)(u)}$  which are stored as  $\hat{\mathbf{X}}^{(2)(r)} = [\hat{x}(0), \dots, \hat{x}(U-1), \hat{x}(U)]$  ( $r = 1, \dots, M$ ).

Step 3:  $MP$  kinds of  $\hat{\mathbf{Z}}_u^{(N-U+1)}$  are obtained by repeating step 2 ( $N-U$ ) times. Finally, the vector  $\hat{\mathbf{X}}^{(N-U+1)(1)}$ , which is the minimum Euclidian distance, is the desired result.

#### IV. PERFORMANCE EVALUATION AND DISCUSSION

##### A) Proposed receiver for the non-multipath fading channel

The  $P_{fa}$  versus threshold and BER performance versus threshold are described in Fig. 2. The proposed system can obtain better performance than that of the conventional blanking system in certain range. For example, Fig. 2(a) shows that the best BER of the conventional blanking system is  $9.4 \times 10^{-5}$ , whereas the best BER of the proposed system is  $7.8 \times 10^{-8}$  (i.e.  $N = 128$ ). Thus, in Fig. 2(b), the BER of the proposal can reach  $2.0 \times 10^{-4}$  (i.e.  $N = 128$ ) compared to that of the conventional blanking system whose BER is  $5.4 \times 10^{-3}$  in the optimal threshold. The numerous simulated results showed that it is the optimal threshold when  $P_{fa}$  is about  $1.0 \times 10^{-3}$  (i.e.  $q = 0.01$ ) and  $P_{fa}$  is about  $1.0 \times 10^{-2}$  (i.e.  $q = 0.1$ ) given  $E_b/N_0 = 20$  dB. Implicitly, the proposed system has best BER value with  $P_{fa} = 1.0 \times 10^{-3}$  in Fig. 3(a) and  $P_{fa} = 1.0 \times 10^{-2}$  in Fig. 3(b) when  $E_b/N_0 = 20$  dB. In addition, the BER performance with  $N = 128$  is better than that of  $N = 64$  in both systems.

Figure 3 shows the performance of the proposed system over the non-multipath fading channel. The proposed system can obtain better performance compared to that of the conventional with or without blanking and clipping process. For example, in Fig. 3(a), the proposed system can obtain about 10 dB  $E_b/N_0$  improvement to achieve  $BER = 1.9 \times 10^{-5}$  when  $P_{fa} = 0.001$ . On the other hand, the curve in Fig. 3(b) is increasing upward after  $E_b/N_0 = 15$  dB, but it is still better than that of the conventional system. The reason is that when  $E_b/N_0$  becomes larger, the power of the Gaussian noise becomes smaller, however the IN and the expected signal are mixed due to large  $\alpha$  although

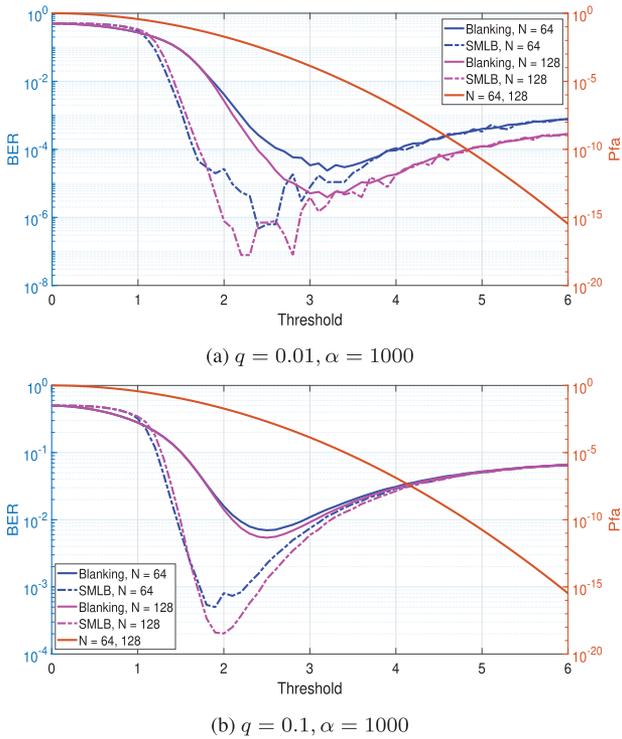


Fig. 2.  $P_{fa}$  versus threshold, BER performance versus threshold for comparison of the conventional blanking system and the proposed system without CFAR detector in the non-multipath fading channel with  $q = 0.01, 0.1$  and  $\alpha = 1000$  given  $E_b/N_0 = 20$  dB when  $N = 64, 128$ . (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .

the expected signal can be separated from the background noise. In addition, the performance of the OFDM with blanking may be better than that of OFDM with clipping (e.g. Fig. 3(b)) which has similar conclusion to [15]. Note that SML itself does not have an impact on the performance in IN environment. As a matter of fact, Hou and Hase [21] have mentioned that a partial duration of the OFDM symbols (i.e. add zeros at the end of the received partial signal) can be recovered by SML under the assumption of only AWGN noise exists. Namely, the combination of SML and zero addition which is used to replace the missing part can improve the performance in the AWGN noise. In our case, the blanked part which is regarded as the IN is set to zero (i.e. the other part is only affected by AWGN), SML recovers the blanked signal.

Figure 4 shows the BER performance of the proposed system versus conventional with and without blanking system when  $q = 0.1$  and different  $\alpha$ . The simulated results show that the proposed system has more ability to improve the performance with increasing  $\alpha$  compared to that of the conventional system. When  $\alpha$  is small, namely, it is difficult to distinguish the difference between the symbols affected by only background noise or IN. The OFDM with blanking and the proposed system cannot mitigate the impact of the IN. However, when  $\alpha$  is large, the proposed system can further improve the BER performance of the OFDM with the blanking system. In addition, generally, moderate or high  $q$  and  $\alpha$  are more valuable to discuss since IN is a dominant factor to affect the performance of the system.

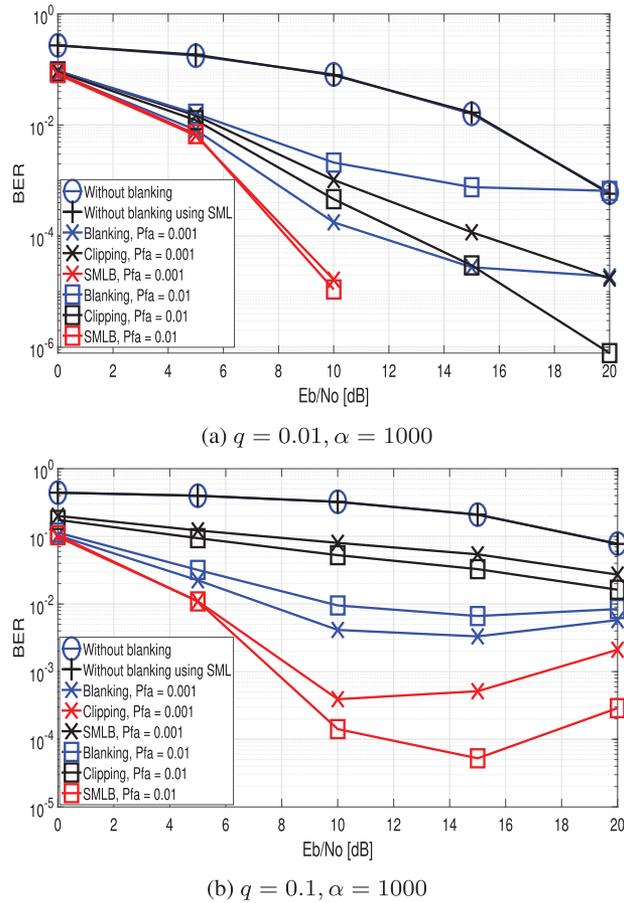


Fig. 3. BER performance versus  $E_b/N_0$  for comparison of the conventional with or without blanking system and the proposed system in the non-multipath fading channel with  $q = 0.01, 0.1$  and  $\alpha = 1000$  given  $P_{fa}$  ( $P_{fa} = 0.001$  and  $0.01$ ). (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .

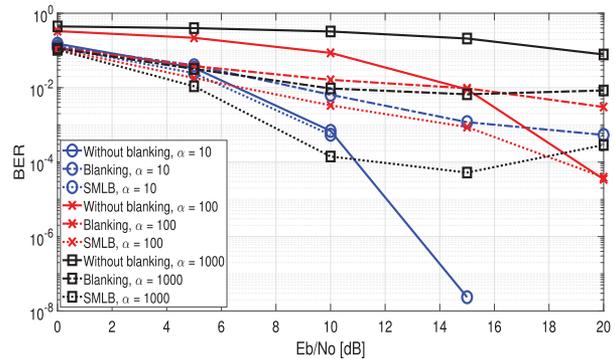
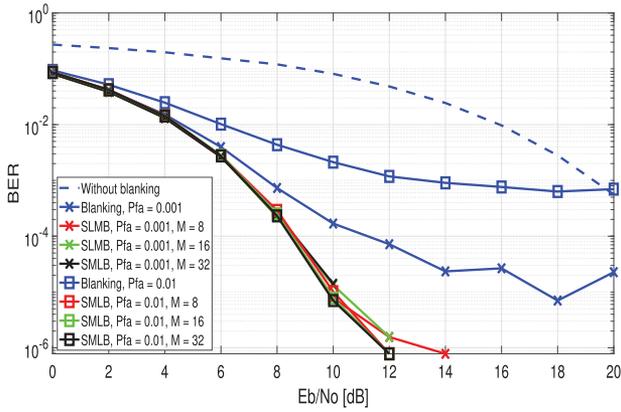
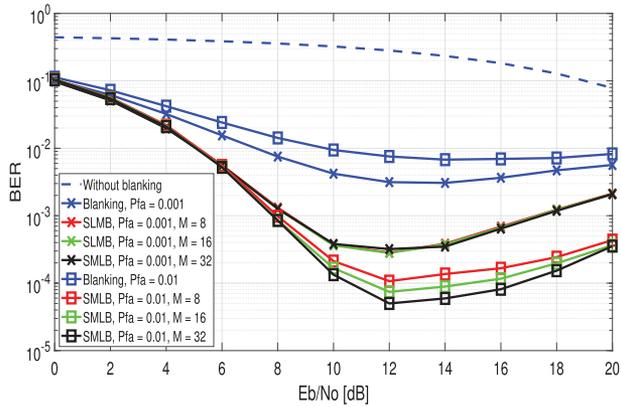


Fig. 4. BER performance versus  $E_b/N_0$  for comparison of the conventional with or without blanking system and the proposed system in the non-multipath fading channel with  $q = 0.1$  and  $\alpha = 10, 100, 1000$  given  $P_{fa} = 0.01$ .

On the other hand, the proposed system can adjust the number of candidates (i.e.  $M = 32$  in this paper) to meet the demand of the trade-off between the BER performance and complexity. The complexity of the proposed system is  $P^{U+k} \times (N - U - k)(MP)$ . Note that  $M$  is the number of the candidates in every iteration,  $P$  is the number of the constellation,  $U$  is the initial number of subcarriers utilized,  $N$  is the number of the subcarriers, and  $k$  is the  $(k + 1)$ th iteration where the number of candidates is less than



(a)  $q = 0.01, \alpha = 1000$

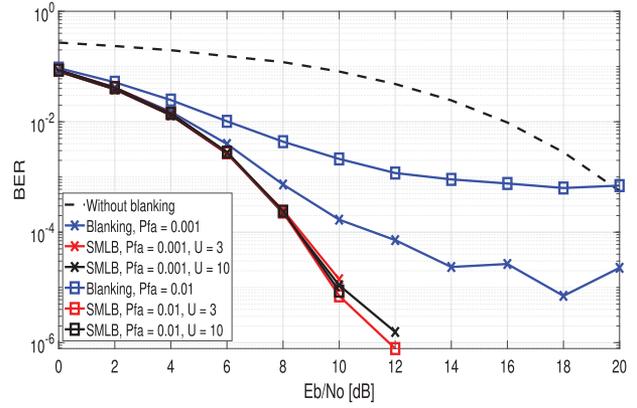


(b)  $q = 0.1, \alpha = 1000$

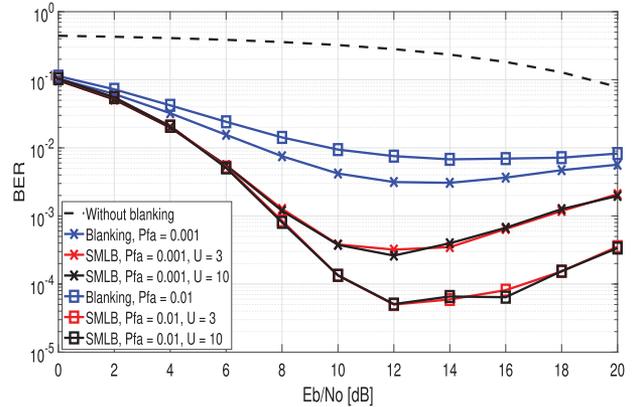
Fig. 5. BER performance versus  $E_b/N_0$  for comparison of the conventional with or without blanking system and the proposed system using different number of candidates ( $M$ ) in the non-multipath fading channel with  $q = 0.01, 0.1$  and  $\alpha = 1000$  given  $P_{fa}$  ( $P_{fa} = 0.001$  and  $0.01$ ) when  $N = 128$ . (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .

$M$ . In this paper, the complexity of the proposed system is  $2^5 \times (123 \times 32 \times 2)$  with  $M = 32, P = 2, N = 128$ , and  $U = 3$ . When  $M = 16$ , the complexity is  $2^4 \times (124 \times 16 \times 2)$  etc. Figure 5(a) shows that when  $q = 0.01, \alpha = 1000$ , the BER performance of the system with  $M = 8, 16$  is almost the same as that of the system with  $M = 32$ . When  $q = 0.1$  as described in Fig. 5(b), the proposed system has worse degradation with  $M$  decreasing (i.e.  $P_{fa} = 0.01$ ), however, the proposed system still has better performance than that of the conventional blanking scheme.

Besides  $M$ ,  $U$  is another parameter of the SML method. When  $U \leq \log_2 M$ , the performance or complexity of system is the same as that of the system with  $U = \log_2 M$ , since the removed possible candidates start from the case that the number of candidates is larger than  $M$ . When  $U > \log_2 M$ , the complexity increases with larger  $U$ . The BER performance versus  $E_b/N_0$  with different  $U$  is described in Fig. 6. The simulated results show that small or moderate  $U$  has no effect on the performance of the system whether moderate or high  $q$  and  $\alpha$ . For high  $U$ , the complexity of the system is approaching to that of the system using MLSE. Therefore, it is not meaningful from the view of SML concept.



(a)  $q = 0.01, \alpha = 1000$



(b)  $q = 0.1, \alpha = 1000$

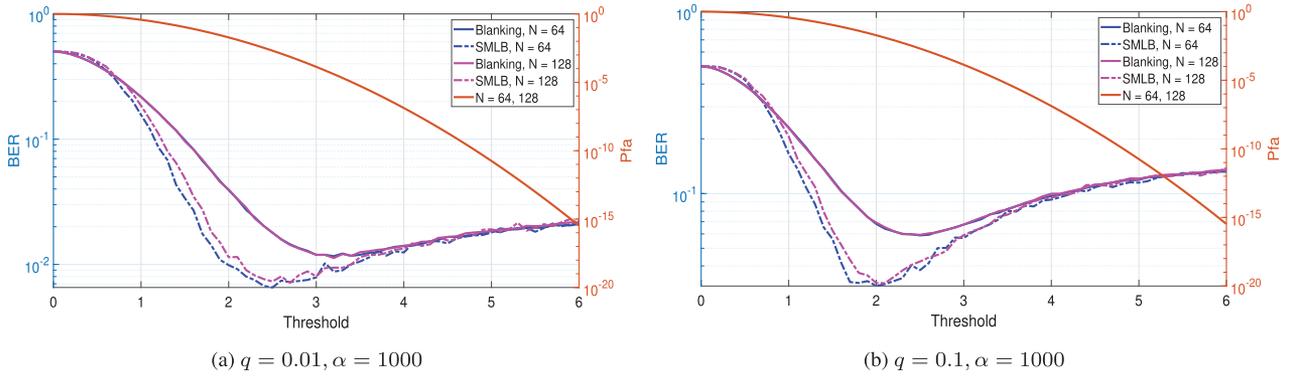
Fig. 6. BER performance versus  $E_b/N_0$  for comparison of the conventional with or without blanking system and the proposed system using different initial number of subcarriers ( $U$ ) in the non-multipath fading channel with  $q = 0.01, 0.1$  and  $\alpha = 1000$  given  $P_{fa}$  ( $P_{fa} = 0.001$  and  $0.01$ ) when  $N = 128$ . (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .

## B) Proposed receiver for the multipath fading channel

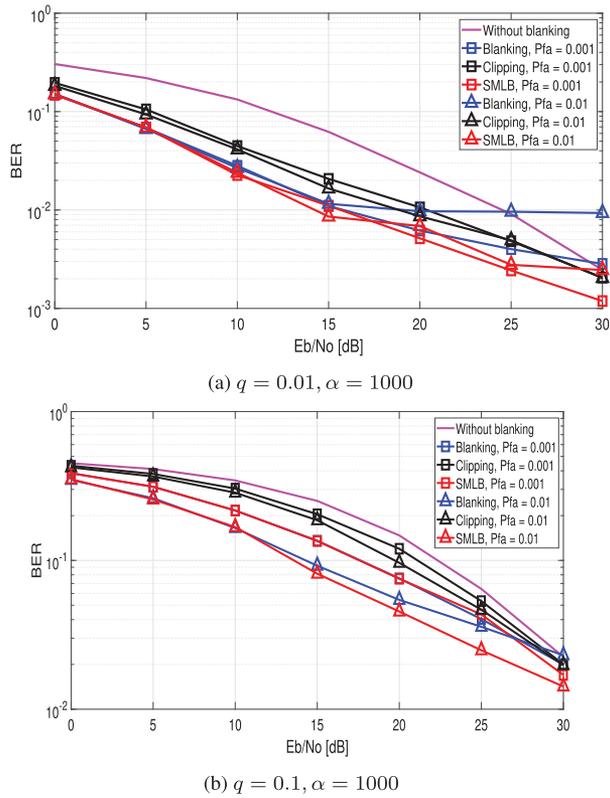
Figure 7 describes the  $P_{fa}$  versus threshold and BER performance versus threshold in the two-path Rayleigh fading channel. The simulated results show that the proposed system can further improve the BER performance of OFDM with blanking when the appropriate threshold is chosen.

The parameter and configuration of the proposed system in the two-path Rayleigh fading channel are shown in Table 1. Figure 8 shows that when  $\alpha = 1000$ , the proposed system has better performance than that of the conventional with or without blanking and clipping system. For example, the proposed system can achieve about 7 dB  $E_b/N_0$  improvement with  $BER = 2 \times 10^{-2}$  given  $P_{fa} = 0.001$  in Fig. 8(a). Therefore, the proposed system can achieve the performance improvement by adjusting  $P_{fa}$  value when  $\alpha$  is very large.

Figure 9 describes the performance of the proposed system with  $\alpha$  varying in the fading channel. When  $\alpha = 10$ , blanking method is not useful, however, SMLB method can improve the performance of the blanking. When  $\alpha = 100$ , the performance is close to that of the system without blanking. The proposed system can achieve about 5 dB



**Fig. 7.**  $P_{fa}$  versus threshold, BER performance versus threshold for comparison of the conventional blanking system and the proposed system without CFAR detector in the two-path Rayleigh fading channel with  $q = 0.01, 0.1$  and  $\alpha = 1000$  given  $E_b/N_0 = 20$  dB when  $N = 64, 128$ . (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .



**Fig. 8.** BER performance versus  $E_b/N_0$  for comparison of the conventional with or without blanking system and the proposed system in the two-path Rayleigh fading channel with  $q = 0.01, 0.1$  and  $\alpha = 10, 1000$  given  $P_{fa} (P_{fa} = 0.001 \text{ and } 0.01)$ . (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .

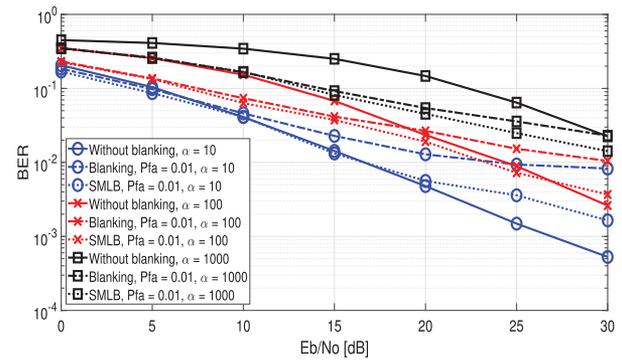
$E_b/N_0$  improvement with  $BER = 2 \times 10^{-2}$  given  $P_{fa} = 0.01$  when  $\alpha = 1000$ . Therefore, the proposed system is able to obtain better performance than that of the system with or without blanking.

In Fig. 10, the performance of the proposed system with  $M = 8$  is almost the same as that of the system with  $M = 32$  whether  $q = 0.01$  or  $q = 0.1$ . Therefore, the complexity can be further reduced compared to that of the system with  $M = 32$  in the Rayleigh fading channel.

**Table 1.** Parameter and configuration of the proposed system

Parameter	Configuration
FFT size	128
Number of symbols	10
CP	32
Modulation	BPSK
$q$	0.01, 0.1
$\alpha$	1000
Channel model	Two-path Rayleigh fading channel
Noise model	BG noise model
Channel estimation	Perfect channel estimation
SML ( $U, M$ )	(3, 32)

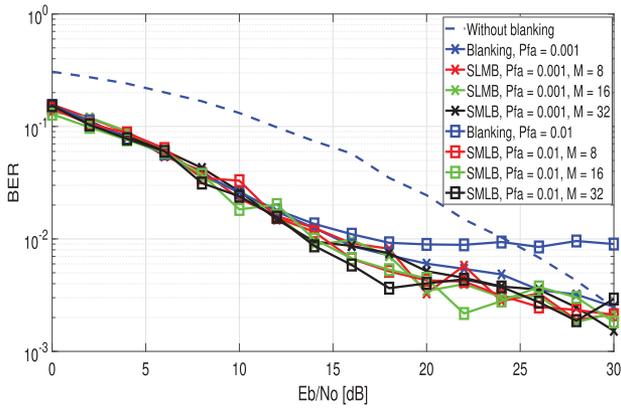
( $U, M$ ):  $U$  is the number of subcarriers used in the first iteration and  $M$  is the number of the candidate values in every iteration.



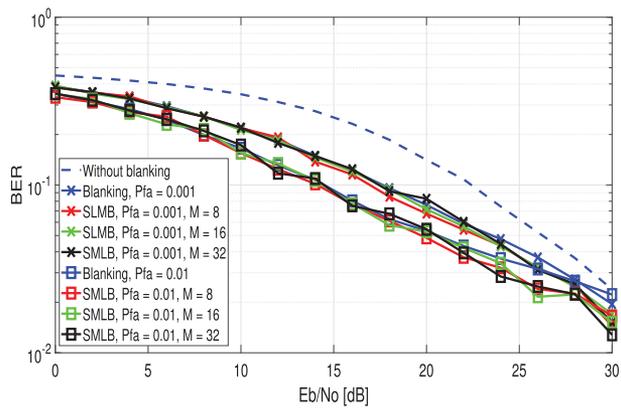
**Fig. 9.** BER performance versus  $E_b/N_0$  for comparison of the conventional with or without blanking system and the proposed system in the two-path Rayleigh fading channel with  $q = 0.1$  and  $\alpha = 10, 100, 1000$  given  $P_{fa} (P_{fa} = 0.01)$ .

### C) Application of the proposed receiver in the 5G systems

Juwono *et al.* [6] show that IN besides background noise is also one of the factors which affects the performance of the system in a harsh industrial factory which requires low latency and high reliability, namely, it refers to the URLLC which is mainly utilized for automatic factory, real-time remote control [28]. It is challenging since IN results in the



(a)  $q = 0.01, \alpha = 1000$



(b)  $q = 0.1, \alpha = 1000$

**Fig. 10.** BER performance versus Eb/No for comparison of the conventional with or without blanking system and the proposed system using different number of candidates ( $M$ ) in the two-path Rayleigh fading channel with  $q = 0.01, 0.1$  and  $\alpha = 1000$  given  $P_{fa}$  ( $P_{fa} = 0.001$  and  $0.01$ ) when  $N = 128$ . (a)  $q = 0.01, \alpha = 1000$ . (b)  $q = 0.1, \alpha = 1000$ .

high BER which causes the problem of the connectivity reliability and severe transmission latency in the event of packet loss. As a matter of fact, OFDM can cope well with the IN when the noise power is moderate. However, IN results in the more errors even OFDM system in the high probability of IN occurrence (high  $q$ ) and high IN power (i.e. it is proportional to  $\alpha$ ). The simulated results showed that the proposed system can further improve the performance of the conventional blanking system even if the probability of IN occurrence and IN power are very high (e.g.  $q = 0.1$  and  $\alpha = 1000$ ) at the same time. Therefore, the proposed system is useful to mitigate the degradation of the system in harsh industrial factory at the acceptable cost of the complexity.

## V. CONCLUSION

In this paper, we proposed an SMLB-based OFDM receiver to mitigate the impact of the IN. The simulated results showed that the proposed system can further improve the performance of OFDM with blanking for high frequent IN occurrence (high  $q$ ) and high IN power (large  $\alpha$ ) with appropriate threshold. We pointed out that the proposed

system can achieve the trade-off between the performance and the complexity by adjusting the  $M$  value. It was effective to mitigate the degradation of the system in harsh industrial factory at the acceptable cost of the complexity.

## FINANCIAL SUPPORT

This research received no specific grant from any funding agency, commercial, or not-for-profit sectors.

## CONFLICT OF INTEREST

None.

## REFERENCES

- [1] Cisco IBSG, 2011.
- [2] Osseiran, A., *et al.*: Scenarios for 5G mobile and wireless communications: The vision of the METIS project. *IEEE Commun. Mag.*, **52** (5) (2014), 26–35.
- [3] Rappaport, T.S., *et al.*: Millimeter wave mobile communications for 5G cellular: it will work!. *IEEE Access.*, **1** (2013), 335–349.
- [4] Willig, A.; Matheus, K.; Wolisz, A.: Wireless Technology in Industrial Networks. *Proc. IEEE.*, **93** (6) (2005), 1130–1151.
- [5] Ma, Y.H.; So, P.L.; Gunawan, E.: Performance analysis of OFDM systems for broadband power line communications under impulsive noise and multipath effects. *IEEE Trans. Power. Deliv.*, **20** (2) (2005), 674–682.
- [6] Juwono, F.H.; Guo, Q.; Huang, D.; Wong, K.P.: Deep clipping for impulsive noise mitigation in OFDM-based power-line communications. *IEEE Trans. Power Deliv.*, **29** (3) (2014), 1335–1343.
- [7] Shhab, L.M.H.; Rizaner, A.; Ulusoy, A.H.; Amca, H.: Impact of impulsive noise on millimeter wave cellular systems performance, in *2017 10th UK-Europe-China Workshop on Millimetre Waves and Terahertz Technologies (UCMMT)*, Liverpool, 2017, 1–4.
- [8] Cheffena, M.: Industrial wireless communications over the millimeter wave spectrum: opportunities and challenges. *IEEE Commun. Mag.*, **54** (9) (2016), 66–72.
- [9] Shafi, M., *et al.*: 5G: a tutorial overview of standards, trials, challenges, deployment, and practice. *IEEE J. Sel. Areas. Commun.*, **35** (6) (2017), 1201–1221.
- [10] Popovski, P.; Trillingsgaard, K.F.; Simeone, O.; Durisi, G.: 5G wireless network slicing for eMBB, URLLC, and mMTC: a communication-theoretic view. *IEEE Access*, **6** (2018), 55765–55779.
- [11] Takada, M.; Saito, M.: Transmission system for ISDB-T. *Proc. IEEE*, **94** (1), 2006, 251–256.
- [12] Andrews, J.G., *et al.*: What will 5G be?. *IEEE J. Sel. Areas Commun.*, **32** (6), 2014, 1065–1082.
- [13] Ghosh, M.: Analysis of the effect of impulse noise on multicarrier and single carrier QAM systems. *IEEE Trans. Commun.*, **44** (2) (1996), 145–147.
- [14] Tseng, D.; Han, Y.S.; Mow, W.H.; Chang, L.; Vinck, A.J.H.: Robust clipping for OFDM transmissions over memoryless impulsive noise channels. *IEEE Commun. Lett.*, **16** (7) (2012), 1110–1113.
- [15] Zhidkov, S.V.: Analysis and comparison of several simple impulsive noise mitigation schemes for OFDM receivers. *IEEE Trans. Commun.*, **56** (1) (2008), 5–9.

- [16] Suraweera, H.A.; Chai, C.; Shentu, J.; Armstrong, J.: Analysis of impulse noise mitigation techniques for digital television systems, in *Proc. 8th International OFDM Workshop*, 2003, 172–176.
- [17] Zhidkov, S.V.: Performance analysis and optimization of OFDM receiver with blanking nonlinearity in impulsive noise environment. *IEEE Trans. Veh. Technol.*, **55** (1) (2006), 234–242.
- [18] Epple, U.; Schnell, M.: Adaptive threshold optimization for a blanking nonlinearity in OFDM receivers, in *2012 IEEE Global Communications Conference (GLOBECOM)*, Anaheim, CA, 2012, 3661–3666.
- [19] Miyamoto, S.; Katayama, M.; Morinaga, N.: Performance analysis of QAM systems under class A impulsive noise environment. *IEEE Trans. Electromagn. Compat.*, **37** (2) (1995), 260–267.
- [20] Takahashi, S.; Hamamura, M.; Tachikawa, S.: A demodulation complexity reduction method using M-algorithm for high compaction multi-carrier modulation systems, in *Proc. IEEE ISWCS 2004*, Mauritius, 2004.
- [21] Hou, Y.F.; Hase, T.: Collision-recovery method for collided OFDM based packets, in *2008 IEEE 19th International Symposium on Personal, Indoor and Mobile Radio Communications*, Cannes, 2008, 1–6.
- [22] Skolnik, M.: *Introduction to Radar Systems*, McGraw-Hill, New York, 2000.
- [23] Zahedpour, S.; Ferdosizadeh, M.; Marvasti, F.; Mohimani, G.; Babaie-Zadeh, M.: A novel impulsive noise cancellation based on successive approximations, in *Proceedings of SampTa 2007*, 2007, 126–131.
- [24] Zahedpour, S.; Feizi, S.; Amini, A.; Ferdosizadeh, M.; Marvasti, F.: Impulsive noise cancellation based on soft decision and recursion. *IEEE Trans. Instrum. Meas.*, **58** (8) (2009), 2780–2790.
- [25] Fernandes, V.; Finamore, W.A.; Ribeiro, M.V.; Marina, N.; Karamachoski, J.: Bernoulli–Gaussian distribution with memory as a model for power line communication noise, in *Proc. Braz. Telecommun. Signal Process. Symp.*, 2017, 328–332.
- [26] Shongwey, T.; Vinck, A.J.H.; Ferreira, H.C.: On impulse noise and its models, in *18th IEEE International Symposium on Power Line Communications and Its Applications*, Glasgow, 2014, 12–17.
- [27] Curuk, S.M.: Impulsive noise models used in power line communications. *Balkan J. Electr. Comp. Eng.*, **7** (2) (2019), 115–122.
- [28] Durisi, G.; Koch, T.; Popovski, P.: Toward massive, ultra reliable, and low-latency wireless communication with short packets. *Proc. IEEE*, **104** (9) (2016), 1711–1726.

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