

RESEARCH PAPER

Tensorial metasurface antennas radiating polarized beams based on aperture field implementation

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This paper presents a procedure for the design of tensorial metasurface antennas radiating polarized beams through aperture field synthesis. The aperture field is generated using the surface wave to leaky wave conversion resulting from metasurface modulation. The design procedure of the feeder is presented with a description of the geometrical parameters affecting the antenna matching. Numerical solutions for single beam and multi-beam metasurface antennas working respectively, at 12.25 and 20 GHz are presented. In addition, a metasurface prototype working at 12.25 GHz is manufactured and measured.

Keywords: Antenna design, Modeling and measurements, Meta-materials and photonic bandgap structures

Received 24 July 2017; Revised 17 October 2017; Accepted 26 October 2017; first published online 23 November 2017

I. INTRODUCTION

In recent years, great interest was given to the realization of low-cost light antennas with high performances in order to extend their use to the public sector. Among the possible candidates, modulated metasurface antennas give interesting performances with a relatively low cost and complexity of production. Metasurfaces are two-dimensional structures consisting of sub-wavelength elements, printed over a grounded dielectric slab. By acting on the size, shape, and orientation of the printed elements, the metasurfaces are modulated. Several examples of such modulated metasurfaces have been designed and presented in the literature [1–7].

The propagation of surface waves (SW) along metasurfaces can be controlled by introducing a modulation of the metasurfaces. In addition, a proper choice of the modulation parameters leads to the generation of radiated leaky-waves (LW) propagating away from the metasurface. Moreover, the metasurface modulation parameters can be used to control the properties of the generated LW (amplitude, phase, and polarization). In [7–9], a method for the generation of aperture field distributions using modulated tensorial metasurfaces was presented. In these articles, a wide range of radiation pattern was achieved with a validation using numerical simulations.

This paper is an extension of [9] for which feeder design and experimental results have been added. In Section II, the

theoretical procedure for the generation of aperture field distributions using modulated metasurfaces presented in [7] is resumed. Section III presents the design procedure of the feeder as well as the geometrical parameters affecting the antenna matching. In Section IV, the aperture generation procedure is validated through numerical simulation of a single beam and a multi-beam metasurface antenna working at 12.25 and 20 GHz, respectively. Simulation results are compared with theoretical radiation patterns. Finally, a metasurface prototype, operating at the frequency $f = 12.25$ GHz, is manufactured and measured in Section V. Conclusions are drawn in Section VI.

II. FORMULATION

The general geometry is depicted in Fig. 1. A feeder excites a cylindrical surface wave propagating above a metasurface realized by printed conducting elements above a grounded dielectric substrate. The physical properties of the metasurface are described in terms of equivalent surface tensorial impedance \underline{Z}_s . This latter is defined as the ratio between tangential electric (E_t) and the magnetic (H_t) fields at the surface boundary S , namely:

$$\mathbf{E}_t(\boldsymbol{\rho}')|_{\boldsymbol{\rho}' \in S} = \underline{Z}_s \hat{\mathbf{n}} \times \mathbf{H}_t(\boldsymbol{\rho}')|_{\boldsymbol{\rho}' \in S} = \underline{Z}_s \mathbf{J}(\boldsymbol{\rho}'), \quad (1)$$

where $\boldsymbol{\rho}' = x' \hat{\mathbf{x}} + y' \hat{\mathbf{y}}$ is a point on the antenna surface, $\hat{\mathbf{n}}$ is the vector normal to the surface S , and $\mathbf{J}(\boldsymbol{\rho}') = \hat{\mathbf{n}} \times \mathbf{H}_t(\boldsymbol{\rho}')|_{\boldsymbol{\rho}' \in S}$ is the equivalent surface current.

Under the assumption that the metasurface is composed of reciprocal and lossless materials, the surface impedance is a

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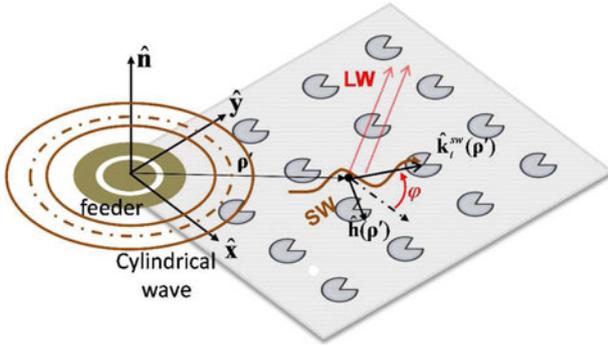


Fig. 1. Metasurface geometry and LW generation.

purely imaginary symmetric tensor [10]. Thus, equation (1) reduces to:

$$\begin{bmatrix} E_1 \\ E_2 \end{bmatrix} = j \begin{bmatrix} X_{11} & X_{12} \\ X_{12} & X_{22} \end{bmatrix} \begin{bmatrix} J_1 \\ J_2 \end{bmatrix} \quad (2)$$

For this kind of structures, the dominant mode is a hybrid EH surface wave mode [11]. The magnetic field above the metasurface will be of the general form [7]:

$$\mathbf{H}_t(\boldsymbol{\rho}') = I(\boldsymbol{\rho}') e^{-jk^{sw}(\boldsymbol{\rho}') \cdot \boldsymbol{\rho}'} \hat{\mathbf{h}}(\boldsymbol{\rho}') \quad (3)$$

where I is the field amplitude, $\hat{\mathbf{h}}$ is the magnetic field polarization unit vector, $\mathbf{k}^{sw} = k_t^{sw} \hat{\mathbf{k}}^{sw}$ and k_t^{sw} are the wave vector and the propagation constant, respectively.

The propagation constant k_t^{sw} is obtained using transverse resonance technique [11, 12]. It should be noted that $\underline{\mathbf{Z}}_s$ depends on the considered wavenumber and propagation direction, namely

$$\mathbf{k}^{sw} = k_t^{sw}(\omega, \varphi)(\hat{\mathbf{x}} \cos(\varphi) + \hat{\mathbf{y}} \sin(\varphi)), \quad (4)$$

where $k_{sw}(\omega, \varphi)$ is the wavenumber associated with the dominant mode propagating along the direction $\hat{\mathbf{k}}_t^{sw}$ defined by the angle φ (Fig. 1) at the angular velocity ω .

A sinusoidal modulation of the surface reactance components along the direction of propagation leads to the generation of an infinite number of Floquet-modes [12]. We consider a reactance components variation of the form :

$$X_{ij}(x) = \bar{X}_{ij} \left[1 + M_{ij} \cos\left(\frac{2\pi}{p_{ij}} x\right) \right], \quad (5)$$

where \bar{X}_{ij} , M_{ij} , and p_{ij} are the average reactance, the modulation index and the periodicity of the ij component, respectively.

For small modulation indices, modes of order -1 are predominant [12]. Under this condition, LW can be generated if the quantity $k_t^{sw} - (2\pi/p_{ij})$ is smaller than the free space propagation constant k_o . The generated LW will then have

the following form [7]:

$$\mathbf{E}_t^{LW} = \begin{bmatrix} E_1^{LW} \\ E_2^{LW} \end{bmatrix} = j \begin{bmatrix} \frac{M_{11}}{2} \bar{X}_{11} J_1 e^{-j\frac{2\pi}{p_{11}} x} + \frac{M_{12}}{2} \bar{X}_{12} J_2 e^{-j\frac{2\pi}{p_{12}} x} \\ \frac{M_{21}}{2} \bar{X}_{21} J_1 e^{-j\frac{2\pi}{p_{21}} x} + \frac{M_{22}}{2} \bar{X}_{22} J_2 e^{-j\frac{2\pi}{p_{22}} x} \end{bmatrix}, \quad (6)$$

A) Aperture field generation:

The idea is to control this LW using the modulation parameters as proposed in [7], in order to generate an arbitrary objective aperture field distribution of the form:

$$\mathbf{E}_t^{obj} = \begin{bmatrix} |E_1^{obj}| e^{j \arg(E_1^{obj})} \\ |E_2^{obj}| e^{j \arg(E_2^{obj})} \end{bmatrix} = \begin{bmatrix} |E_1^{obj}| \Psi_1^{obj} \\ |E_2^{obj}| \Psi_2^{obj} \end{bmatrix} = |\mathbf{E}_t^{obj}| \Psi_{obj}. \quad (7)$$

The phase distribution of the LW is controlled by acting on the periodicity of the modulation using holography principle. The holography principle is applied in a local framework formulation in order to obtain the desired phase distribution while at the same time ensuring the anti-Hermitian property of the impedance tensor [7]. This leads to the following condition:

$$\underline{\mathbf{Z}}_s(\boldsymbol{\rho}') = \underline{\mathbf{R}}(\boldsymbol{\rho}')^{-1} \begin{bmatrix} X_{11}^{loc} & X_{21}^{loc} \\ X_{21}^{loc} & X_f \end{bmatrix} \underline{\mathbf{R}}(\boldsymbol{\rho}'), \quad (8)$$

where $X_{n1}^{loc} = \bar{X}_{n1}^{loc} \left[1 + M_{n1}^{loc} \mathfrak{S}(\Psi_{obj,n}^{loc} \cdot \Psi_{inc,1}^{loc*}) \right]$, the *loc* superscript indicates that the quantity is written in the local framework, $\underline{\mathbf{R}}(\boldsymbol{\rho}')$ is the transformation matrix between the local and the global framework, and X_f is a free parameter [7].

Equation (8) is obtained by defining the *incident phase wave* Ψ_{inc} as the phase of the current \mathbf{J} , and the *objective phase wave* Ψ_{obj} .

Then, each amplitude component is obtained imposing the product between the modulation index and the average impedance to be proportional to $|E_i^{obj}|$, yielding [7]:

$$\begin{cases} \bar{X}_{11}^{loc}(\boldsymbol{\rho}') M_{11}^{loc}(\boldsymbol{\rho}') |H_2^{loc}(\boldsymbol{\rho}')| \propto |E_{obj,1}^{loc}(\boldsymbol{\rho}')| \\ \bar{X}_{12}^{loc}(\boldsymbol{\rho}') M_{12}^{loc}(\boldsymbol{\rho}') |H_2^{loc}(\boldsymbol{\rho}')| \propto |E_{obj,2}^{loc}(\boldsymbol{\rho}')| \end{cases}. \quad (9)$$

B) Objective aperture field calculation

In this paper, we focus on the generation of single or multiple beams with arbitrary polarizations and directions of radiation. A single linearly polarized beam pointing at θ_o , ϕ_o can be obtained using the following aperture distribution [7-9]:

$$\mathbf{E}_t^{obj}(\boldsymbol{\rho}') = e^{-jk_o(\sin \theta_o \cos \phi_o x' + \sin \theta_o \sin \phi_o y')} \hat{\mathbf{e}}(\phi_o), \quad (10)$$

where the amplitude is constant over the aperture and the

polarization of the radiated beam is controlled by $\hat{e}(\phi_o)$ as:

$$\hat{e}(\phi_o) = \begin{cases} \cos \phi_o \hat{x} + \sin \phi_o \hat{y} & \text{for } \hat{\theta} \text{ polarization} \\ -\sin \phi_o \hat{x} + \cos \phi_o \hat{y} & \text{for } \hat{\phi} \text{ polarization} \end{cases} \quad (11)$$

A circularly polarized beam can then be generated by superposing two orthogonal linearly polarized beams with a $\pi/2$ phase shift. In addition, multiple beams can be obtained by superposing the field distribution corresponding to each desired beam. This leads to [7–9]:

$$\mathbf{E}_t^{obj}(\boldsymbol{\rho}') = \frac{1}{N_{beams}} \sum_{k=1}^{N_{beams}} \mathbf{E}_t^k(\boldsymbol{\rho}'), \quad (12)$$

where N_{beams} is the number of beams and $\mathbf{E}_t^k(\boldsymbol{\rho}')$ is the objective field corresponding to each individual beam.

III. METASURFACE IMPLEMENTATION

The surface impedance variation obtained using equations (8) and (9) is implemented using a square lattice of sub-wavelength metallic patches printed over a grounded dielectric substrate [1–9]. The unit cells consist of a circular patch with a v-shaped slot (see Fig. 2). The geometry is described by the following parameters: the spatial periodicity d' , the patch diameter d , the slot width g , and opening angle θ , and the patch rotation ψ . A database of the impedance tensor elements variations with respect to the unit-cell parameters is generated in order to implement the desired reactance distribution.

Figure 3 describes the feeding structure generating the cylindrical wave excitation. The feeder consists of a circular patch of radius r_2 with an annular slot of inner radius r_1 . The slot is also described by its thickness e (Fig. 3(b)).

For a fixed substrate of permittivity ϵ_r and thickness h , the antenna adaptation is influenced by the parameters r_1 , r_2 , and e . The resonant frequency is mainly controlled using the outer radius r_2 . On the other hand, the parameters r_1 and e have more influence on the level of the scattering parameter $|S_{11}|$ at the resonant frequency.

Figure 4 represents the variations of the scattering parameter $|S_{11}|$ in dB with respect to the frequency for different values of the outer radius r_2 . The metasurface is printed on a substrate Rogers TMM6 of thickness 1.27 mm and relative

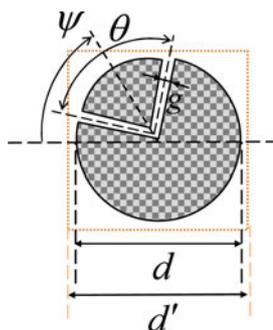


Fig. 2. Unit cell design: circular patch with a v-shaped slot.

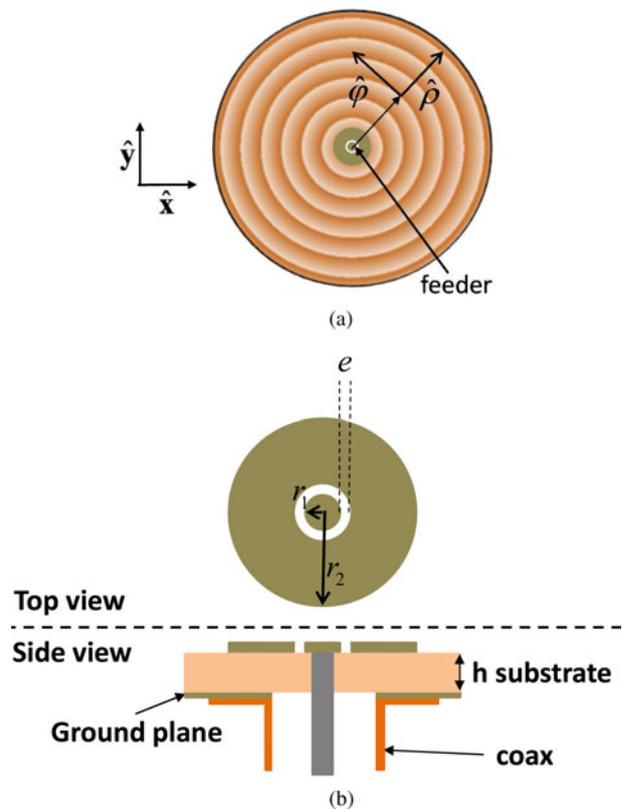


Fig. 3. Structure generating the cylindrical wave excitation. (a) Position of the feeder. (b) Structure of the feeder.

permittivity 6. The curves were simulated using the software HFSS for the parameters $(r_1;e) = (0.8;0.25)$ mm. It can be seen from the figure that the resonant frequency is shifted by varying the parameter r_2 .

In Fig. 5 the variation of the parameter $|S_{11}|$ in dB for different values of the inner radius r_1 is presented. It can be seen from the figure that the parameters mainly affects the level of the scattering parameter at the resonant frequency even though it produces a slight frequency shift. The latter has to be corrected by readjusting the outer radius r_2 . A similar behavior is observed with the parameter e .

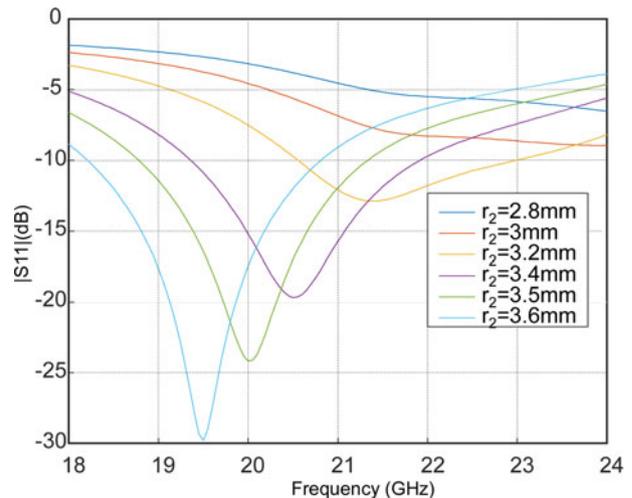


Fig. 4. Metasurface adaptation with respect to the outer radius r_2 for a substrate Rogers TMM6 of permittivity 6 and thickness 1.27 mm.

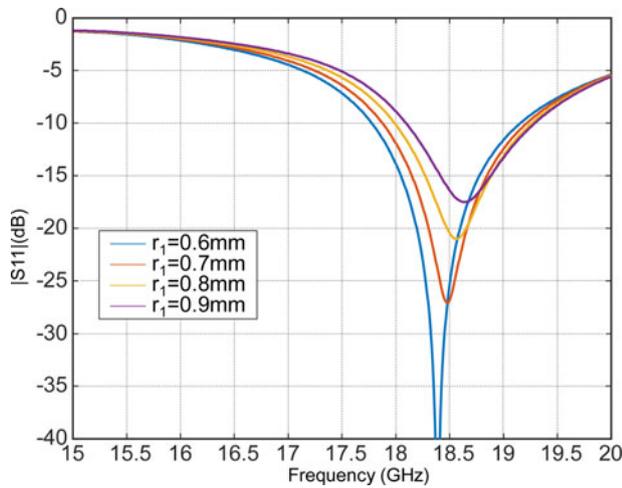


Fig. 5. Metasurface matching with respect to the inner radius r_1 for a substrate Rogers TMM6 of permittivity 6 and thickness 1.27 mm.

IV. NUMERICAL RESULTS

Following the design procedure developed in Sections II and III, two metasurface antennas able to radiate a broadside Right-hand circularly polarized (RHCP) beam at 12.25 GHz and two independent beams at 20 GHz were designed.

The broadside RHCP antenna was designed for a substrate FR4 of thickness 1.6 mm and relative permittivity 4.4 with a diameter of 13λ . The objective aperture field distribution was calculated with MATLAB using equations (10) and (12). Its representation in the cylindrical coordinates is given in Fig. 6. The corresponding local reactance tensor components $X_{11}^{loc}(\rho')$ and $X_{12}^{loc}(\rho')$ are illustrated in Fig. 7.

Using an in-house MATLAB code based on the proposed procedure, the metasurface giving the objective aperture field distribution was generated. The metasurface was then imported in the simulation software ANSYS Designer in order to simulate the radiation pattern. Figure 8 represents the circular components of the simulated far-field radiation

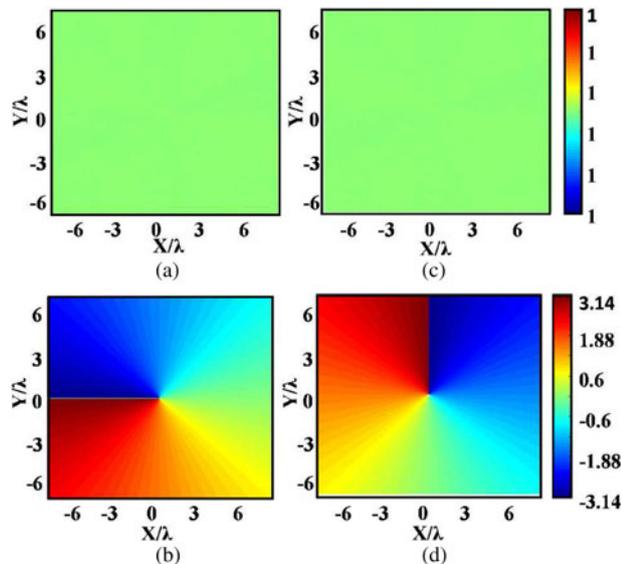


Fig. 6. Aperture field distribution for the broadside RHCP radiation pattern. (a) $|E_{\rho}^{obj}|$; (b) $\arg(E_{\rho}^{obj})$; (c) $|E_{\phi}^{obj}|$; (d) $\arg(E_{\phi}^{obj})$.

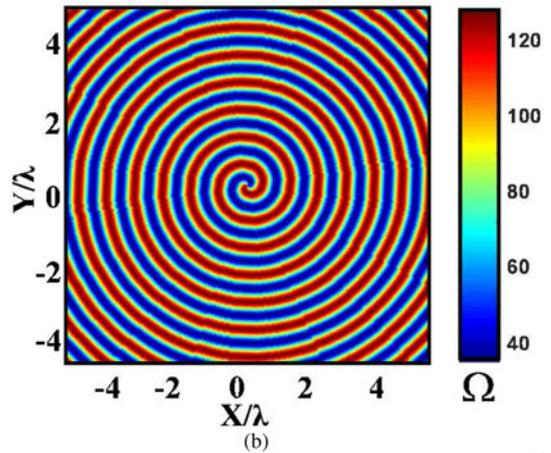
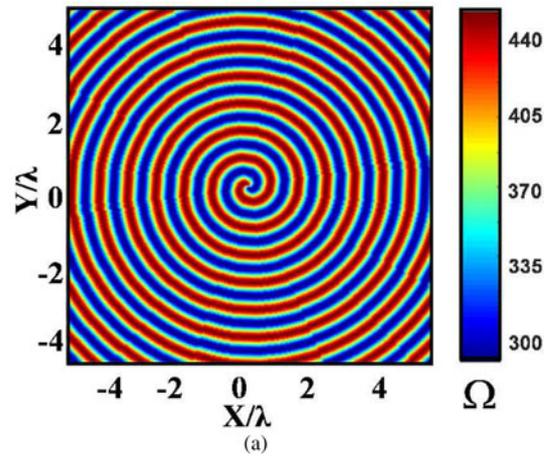


Fig. 7. Variations of the reactance tensor components for a broadside RHCP metasurface. (a) $X_{11}^{loc}(\rho')(\Omega)$; (b) $X_{12}^{loc}(\rho')(\Omega)$.

pattern for the $\phi = 0^\circ$ cut-plane. The left-hand circularly polarized (LHCP) component is represented in red while the RHCP component is represented in blue. We can see from the figure that the metasurface radiates the desired RHCP beam at broadside with a cross-pol level of -30 dB.

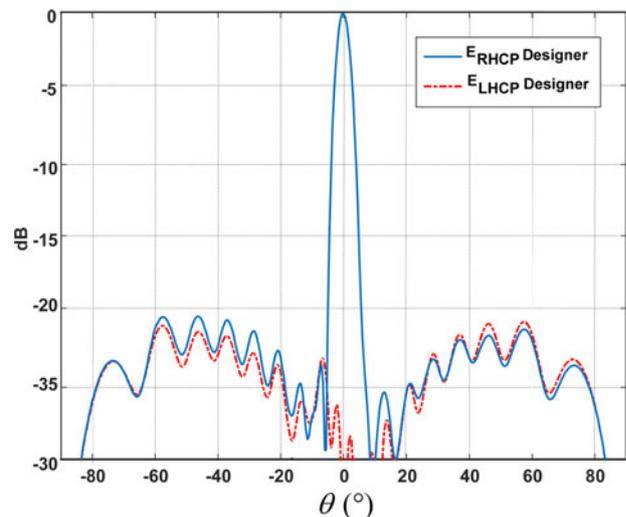


Fig. 8. Far-field radiation pattern (normalized) in dB for the $\phi = 0^\circ$ cut-plane. The RHCP component E_{RHCP} is given in solid line while the LHCP component E_{LHCP} is given in dashed lines.

As a second example, an antenna radiating the first beam at $(\theta_o, \phi_o) = (30^\circ, 0^\circ)$ with linear polarization along the ϕ -axis and a second beam pointing at $(\theta_o, \phi_o) = (45^\circ, 135^\circ)$ with RHCP has been considered.

The metasurface has a radius of 5λ and has been realized printing the conducting elements on a Rogers TMM6 substrate of thickness 1.27 mm and relative permittivity 6. The incident surface wave with a cylindrical wave front was generated using a feeder of parameters $(r_1; r_2; e) = (0.8; 3.5; 0.25)$ mm and placed at the center of the metasurface.

Figure 8 represents the aperture field distribution (phase and amplitude) required to obtain the desired two beams radiation pattern in cylindrical coordinates. The aperture distribution has been calculated with MATLAB using equations (10) and (12).

The corresponding local reactance tensor components $X_{11}^{loc}(\rho')$ and $X_{12}^{loc}(\rho')$ are illustrated in Fig. 9. As it can be seen from Fig. 10, the complexity of the aperture distribution needs a strict control of the phase and amplitude of the generated LW.

A metasurface having the corresponding impedance values has been generated using our in-house MATLAB code and simulated on the software ANSYS Designer. The designed structure is represented in Fig. 11 and the corresponding far-field radiation patterns for the $\phi = 0^\circ$ and $\phi = 135^\circ$ cut-planes are given (in black) in Fig. 12. The simulated radiation pattern is compared with radiation given by the perfect continuous objective aperture field distribution (in blue) and with the free-space radiation resulting from the equivalent magnetic currents (in red).

As can be seen from Fig. 12, the far field radiated by the metasurface antenna corresponds to the objective multi-beam radiation pattern and is in close agreement with the theoretical results. As expected, we obtained the first beam with linear polarization along the ϕ axis, pointing at $\theta = 30^\circ$, $\phi = 0^\circ$, as well as a second beam, with RHCP pointing at $\theta = 45^\circ$ and $\phi = 135^\circ$. The cross-polarization levels are equal to -16 dB for the first beam and -20 dB for the second.

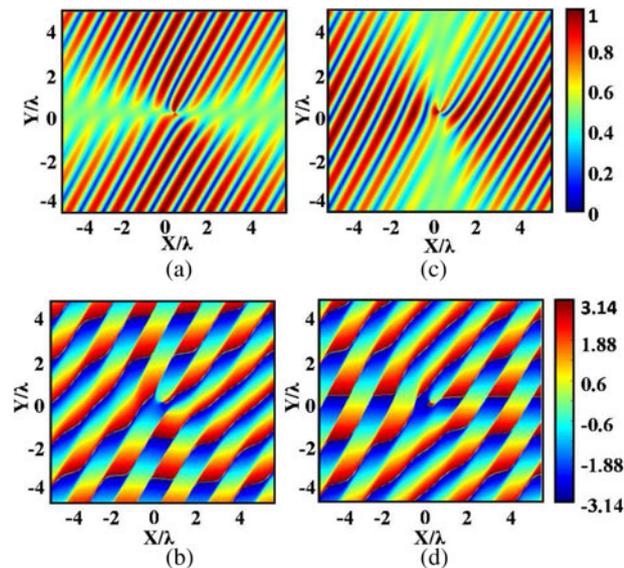


Fig. 9. Aperture field distribution of the two beams metasurface antenna [9]. (a) $|E_\rho^{obj}|$; (b) $\arg(E_\rho^{obj})$; (c) $|E_\phi^{obj}|$; (d) $\arg(E_\phi^{obj})$.

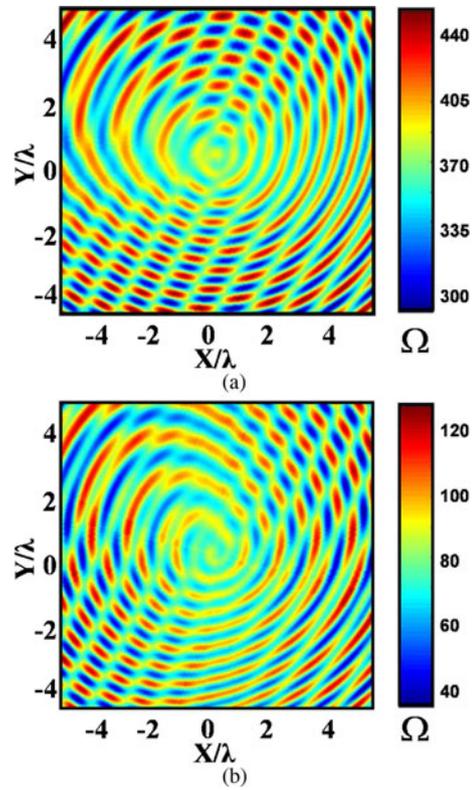


Fig. 10. Variations of the reactance tensor components for a two beams metasurface [9]. (a) $X_{11}^{loc}(\rho')$ (Ω); (b) $X_{12}^{loc}(\rho')$ (Ω).

V. EXPERIMENTAL RESULTS

In this section, a prototype metasurface antenna designed using the presented procedure is measured. The designed antenna radiates a RHCP broadside beam at an operating frequency of 12.25 GHz (Ku band). The manufactured circular metasurface of radius 13λ was printed on a substrate FR4 of thickness 1.6 mm and permittivity 4.4.

For the considered substrate, the antenna is matched with a feeder of parameters $(r_1; r_2; e) = (0.8; 3.5; 0.25)$ mm. Figure 13 presents the measurement and simulation of the variation of the scattering parameter $|S_{11}|$ (dB) with respect to the frequency. The manufactured antenna is represented in the inset of the figure. It can be seen from the figure that the antenna is matched at the desired frequency. In addition, a

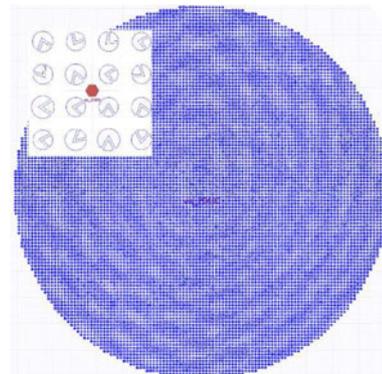


Fig. 11. Metasurface structure on ANSYS Designer.

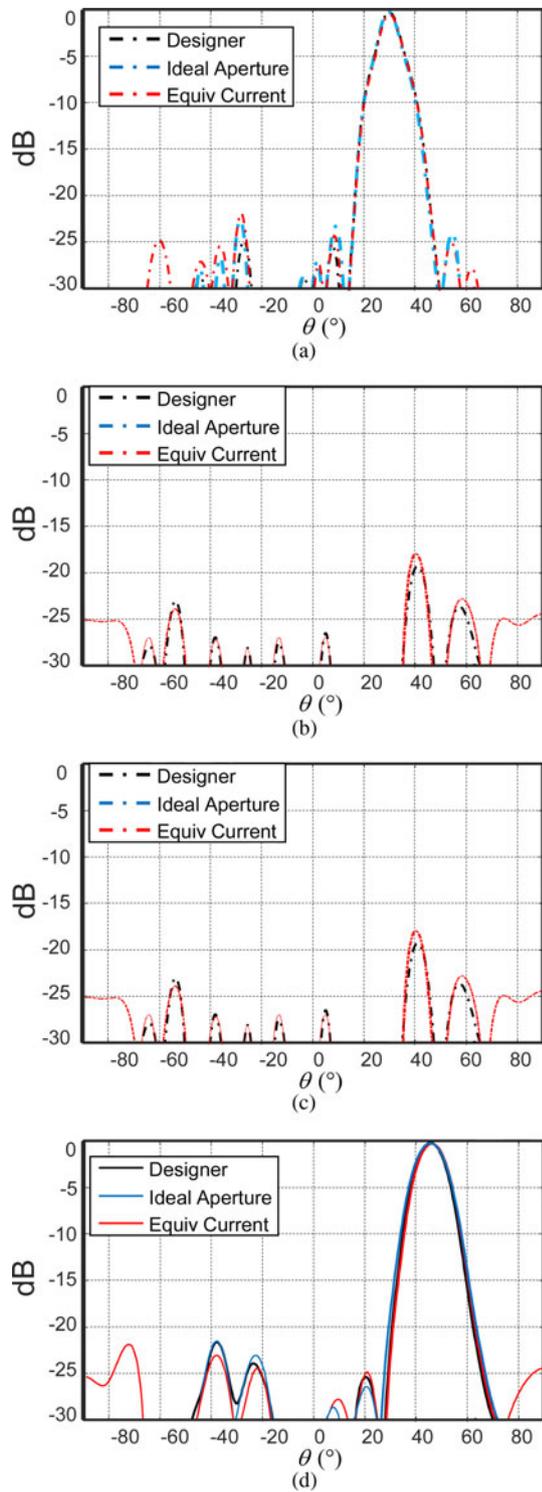


Fig. 12. Far field radiation pattern in dB. (a) $\phi = 0^\circ$ cut-plane E_{ϕ} . (b) $\phi = 0^\circ$ cut-plane E_{θ} . (c) $\phi = 135^\circ$ cut-plane E_{LHCP} . (d) $\phi = 135^\circ$ cut-plane E_{RHCP} .

close agreement is found between the simulation and the measurement.

The far-field radiation pattern of the manufactured antenna was simulated in Designer and measured in the GeePs laboratory in France. The simulated radiation pattern (in red) and the measurement results (in black) for the $\phi = 0^\circ$ cut-plan are presented in Fig. 14 at a working frequency of 12.25 GHz. The RHCP components are represented by solid lines while the LHCP components are presented in dashed

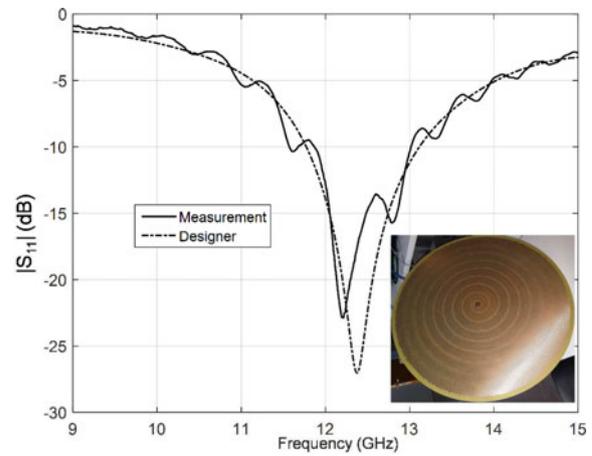


Fig. 13. Simulation and measurement of the scattering parameter $|S_{11}|(dB)$ with respect to the frequency.

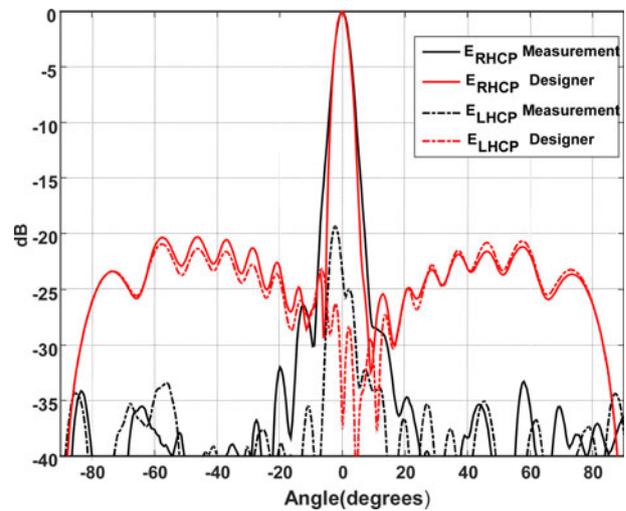


Fig. 14. Simulation (in red) and measurement (in black) of the circular components of the far field radiation pattern (normalized) for the $\phi = 0^\circ$ cut-plan. Solid lines represent RHCP components and dashed lines represents LHCP components. The working frequency is 12.25 GHz.

lines. It can be seen from the figure that the desired RHCP beam is radiated at broadside with a measured cross-pol level of -20 dB. In addition, the measured side lobe level is -27 dB. A close agreement is obtained between the measurement and the simulation in the region of the principal lobe. The discrepancy outside of the lobes is probably due to the fact that the dielectric is assumed infinite in the simulations using Designer. There is a, therefore, discontinuity in the structure at the end of the metasurface. In addition, due to the complexity of the structure, the mesh quality is significantly limited by the computer performances.

VI. CONCLUSION

In this paper, previous work on the generation of aperture field distribution using modulated tensorial metasurface is extended. The design procedure of the feeding structure and the antenna matching parameter are presented. The proposed method is validated with numerical simulations by comparison with theoretical radiation of perfect aperture field distribution.

In addition, an antenna prototype is manufactured and measured giving good agreement with simulations results in term of scattering parameters and radiation pattern.

ACKNOWLEDGEMENT

We wish to thank the CNES (Centre National d'Etudes Spatiales) and Airbus Group Innovations for supporting this project.

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